PN9000
Phase Noise Test System

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PN9000 Phase Noise Measurement System

The Modular design of the PN9000 provides versatility and flexibility to setup the appropriate configuration to measure any kind of frequency source from 2 MHz to 140 GHz.

Techniques:

- Phase Lock Loop
- Delay line (option)
- Added phase noise (option)
- Amplitude Noise (option)

Plug-in optional modules:

- Internal phase detectors up to 40 GHz
- Low Noise Built-in DC FM Reference Synthesizer
- MW down-converters for stable and free-running Sources
- mmW external harmonic mixers/diplexers to extend the frequency coverage up to 140 GHz
- Pulse generator and modulator

Software:

- WPN9000: Windows based graphical user interface with file management
- Remote control option through 10/100/1000 BaseT Ethernet or GPIB

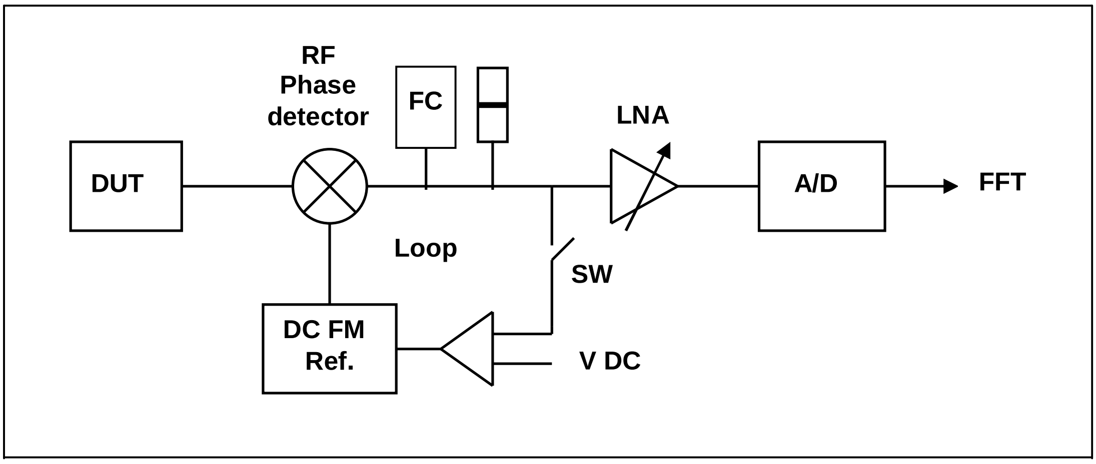
System Controller:

The standard controller is a desktop workstation with USB, printer ports and DVD writer; HDD is 40GB or better, TFT monitor, keyboard and mouse.
Optionally, the desktop can be replaced by an industrial computer.
The operating system is Windows XP pro.

The base system is the core of any measurement configuration. It includes hardware and software, except the reference source, to measure stable sources from 2 MHz to 1.8 GHz.

Note: All the options are described and specified in separate datasheets.

PN9000 System Basic Capabilities



Base System Operating Diagram

Using the built-in frequency counter, in open loop, the DC/FM reference source is manually or automatically tuned on the DUT frequency. The beat signal between DUT and reference is used to measure the demodulation factor of the phase detector using multiples techniques allowing non-linear operation of the detector.

Loop bandwidth and reference FM deviation (or tune slope) will be adjusted depending on the expected noise and stability of the DUT. For most of PLL and synthesizers a few hundred Hz is an average convenient value. Then, closing the loop, the reference source will be phase locked on the DUT signal and RF/LO phase detector inputs will be set automatically in phase quadrature, providing at the output of the detector the combined phase noise of the DUT and the reference. The bar graph located on the lock control module will allow a quick visual check of the loop status (the bar graph should be centered and steady). When the reference’s phase noise is 6 dB better than the DUT’s one, its contribution to the detected noise is 1 dB only.

The LNA, with auto-gain feature, will adjust the noise level to the optimum dynamic range of the digitizing board housed into the computer. FFT calculation process is done in the computer and displayed on the monitor (not represented on the diagram). Loop bandwidth is fully compensated to display phase noise down to 0.01 Hz from the carrier.

In PLL measurements, the system residual noise, or noise floor, will be the reference oscillator’s phase noise.

PN9000 Base System

PN9000 mainframe including:
- Noise output module
- Phase lock control module
- LNA module
- Standard and High level RF phase detectors
- Power Supply

Personal Computer including:
- TFT flat screen monitor
- Digitizing board
- Set of Cables
- OS, Software and manual

PN9000 Base System Specifications

Frequency Input Range : 2 MHz to 1.8 GHz
Offset Analysis : 0.01 Hz to 1 MHz
RF Input Impedance : 50 Ohms
Measurement Accuracy : ± 2 dB up to 1 MHz offset, ± 3 dB above 1 MHz offset
Reference Tuning Voltage : ± 20 Volt with 5mV resolution
Phase Lock Loop Gain : Proportional and Integral (DUT drift compensation)
Loop Compensation : Automatic (can be disabled)

Parameters	**Standard RF**	**High Level RF**
Frequency range, GHz	0.002 to 1.8	0.002 to 1.6
RF Input min. dBm	- 20	+ 10
RF input max. dBm	+ 10	+ 20
LO input min. dBm	0	+ 10
LO input max. dBm	+ 10	+ 20
RF input Gain, dB	-10, 0, 10, 20	None
LO input Gain, dB	0, 10	None
Noise floor, in dBc/Hz at		
1 Hz offset	- 130	- 140
10 Hz	- 140	- 150
100 Hz	- 150	- 160
1 kHz	- 160	- 170
10 kHz	- 168	- 178
100 kHz & beyond	- 168	- 178
Nominal RF input level, dBm	+ 6	+ 16
Nominal LO input level dBm	+ 7	+ 17

For specified values add + 3dB (± 2 dB accuracy). For RF levels < nominal value, the noise floor will increase by the number of dB below the nominal value. For example, for 0 dBm RF input, instead of +6, the typical system residual noise is, at 10 kHz offset : -168 dBc/Hz – 6 dB = – 162 dBc/Hz.

Spurious level : - 110 dBc
Built-in Counter, RF and LO ports : 2MHz to 2 GHz
IF/Beat : 0.3 Hz to 400 kHz

Mechanical Dimensions: PN9000A : HxWxD :13.3 x 38.5 x 68.5 cm or 5.25”x17.72”x26.97”
Power Supply : 100-240 VAC, 50/60 Hz +/- 3%

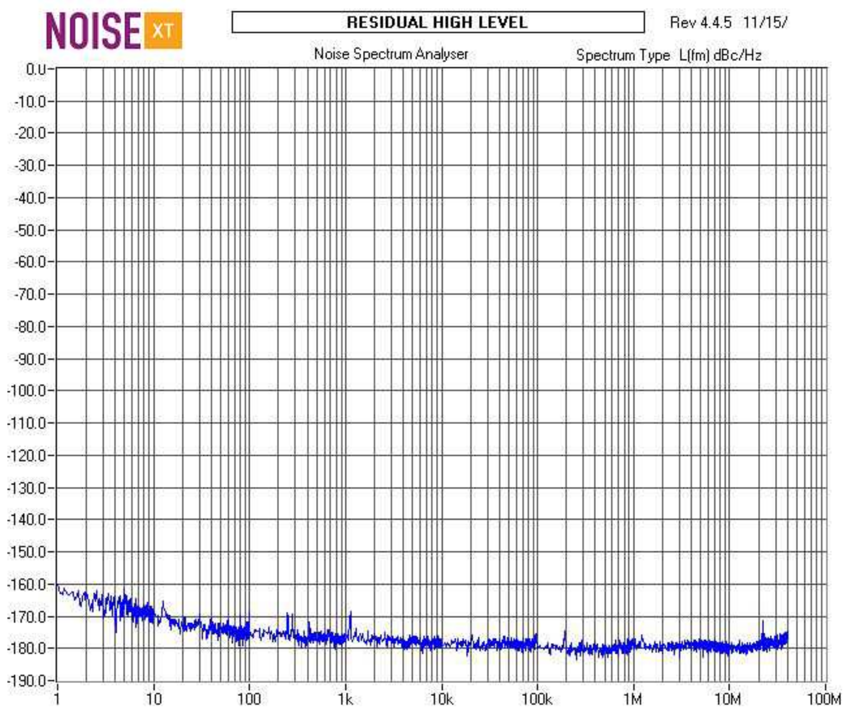
Temperature & Humidity , operating : +10 to + 40 °C
Storage : - 40 to + 75 °C. Up to 95 % non condensing.

PN9000 typical phase and amplitude detectors options Specifications

Parameters	MW (option) Std level	MW (option) High level	MW (option) PN9361-02	MW (option) PN9361-04	AM (option)
Frequency range, GHz	1.6 to 26.5	1.6 to 26.5	5 to 40	1.8 to 50	0.01 to 26.5
RF Input min. dBm	- 10	+ 5	- 10	- 10	- 5
RF input max. dBm	+ 15	+ 20	+ 15	+ 15	+ 15
LO input min. dBm	+ 7	+ 10	+ 7	+ 7	NA
LO input max. dBm	+ 15	+ 23	+ 15	+ 15	NA
RF input Gain, dB	None	None	None	None	None
LO input Gain, dB	None	None	None	None	None
Noise floor, in dBc/Hz at					
1 Hz offset	- 120	- 128	- 125	- 125	NA
10 Hz	- 130	- 138	- 135	- 135	NA
100 Hz	- 140	- 148	- 145	- 145	- 142
1 kHz	- 150	- 158	- 155	- 155	- 150
10 kHz	- 160	- 168	- 168	- 168	- 160
100 kHz & beyond	- 168	- 174	- 168	- 168	- 160
Nominal RF input level, dBm	+ 10	+ 15	+ 10	+ 10	+ 12
Nominal LO input level dBm	+ 10	+ 20	+ 10	+ 10	NA

Notes:

- PN9361-02 and PN9361-04 use K type connectors for RF and LO ports; others use SMA type.
- PN9341-01 and PN9348 modules integrates the MW Std level option
- PN9341-03 integrates the MW High level option
- Minimum pulsed signals duty cycle is 1%



Residual noise with high-level phase detector option

WPN9000 Software

The Windows software provides a friendly interface to the system:

Measurement method control

Selection of measurement method, depending on the DUT

PLL Synth for reference synthesizer method, for stable sources
PLL Xtal for crystal sources
VCO (delay line) for free running sources
AM noise
Noise voltage for voltage sources
ADD NOISE added noise for two port devices
PULSE for pulsed sources or pulsed two ports devices (PM, AM, Added noise)

Photographic based cabling help to guide the user in wiring settings

System configuration, file management, phase detector, frequency range, down-converter, … selections

Store and display up to ten measurements or specifications lines with direct access memories. Plot export as text, BMP or JPEG file to any windows accessible storage device.

Measurement mode - Automatic and Manual

Automatic Measurement are based on embedded expertise that guides the user through the measurement process. In most of the cases, a single click is enough
.
Manual Measurement for reference LO selection and tuning, phase detector calibration factor measurement, loop bandwidth and reference tune slope, reference phase locking

Data processing

Noise/Spurious differentiation	: Spurs expressed and displayed in dBc.
Display functions	: Smooth, spec-line, frequency & level markers, spurs list
Data Computation	: A ± B, N*A, A:N, A±N*B, A±NdB
Integrated power	: in dBc, radian rms, radian^2, degree rms, degree^2, Hz rms, Hz^2
Variance	: Allan,True, Modified and Tvar
Jitter	: Sec_{rms} ,Sec_{pp} ,UI_{pp}
FFT / Spectrum Analysis	: L(f) dBc/Hz, Power dBv^2/Hz, M(f) dBc/Hz
Speed (PN969x-HR options)	: less than 30 seconds for 10 averages (100Hz to 40MHz)
Plot Printing	: Any windows supported printers
External synthesizer driver	: User defined IEEE-488 control menu to set up most of commercial signal generators

PN9100

BUILT-IN LOW NOISE
DC/FM FREQUENCY SYNTHESIZER
2 MHz to 4.5/18 GHz

The reference frequency source is the keystone of easy phase noise measurements with low residual noise and high dynamic range. As a matter of fact, the residual system noise will be that of the reference source, in FM mode, since the base system residual noise is much lower.

Most commercial DC/FM signal generators can be used as the external reference source, controlled from the PN9000 software (through the use of user defined drivers). However, the appropriate signal generator will depend on the expected noise of the DUT. Should the DUT noise be low, close-in or far away from the carrier, the reference synthesizer noise will have to be clean, close-in or far away, accordingly. Unfortunately, most commercial RF signal generators do not provide both close-in and far away low noise. Thus, depending on the DUT applications, two signal generators often have to be used, which is not convenient. It takes too much space and immobilizes an instrument with many functions which are not used for phase noise measurements.

The PN9100 is designed to provide simultaneously low phase noise, close-in and far away from the carrier. It is housed in the PN9000 mainframe; it makes the system smaller, lighter and easier to move.

Optional doublers extend the base frequency range to 9 and 18 GHz. Low frequency synthesis is obtained by dividing the core frequency band (2.048 to 4.380 Ghz). It enables the phase noise to go down to the residual noise of the dividers, about –152 or -155 dBc/Hz. It is often better than many crystal oscillators.

CW and DC FM Range 1 - typical SSB phase noise in dBc/Hz (with standard time base)

Frequency Range, MHz	Slope Hz/V	FM Max	1 Hz	10 Hz	100 Hz	1 kHz	10 kHz	100 kHz	1 MHz	10 MHz
17360 – 18000	3200	FM1	- 30	- 60	- 81	- 103	- 105	- 105	- 124	- 150
8680 – 17360	3200	FM1	- 30	- 60	- 81	- 106	- 112	- 112	- 130	- 150
4340 – 8680	1600	FM1	- 36	- 66	- 87	- 112	- 118	- 118	- 136	- 156
2048 – 4340	800	FM2	- 42	- 72	- 93	- 118	- 124	- 124	- 142	- 162
1024 – 2048	400	FM2	- 48	- 78	- 99	- 124	- 130	- 130	- 148	- 152
512 – 1024	200	FM2	- 54	- 84	- 105	- 130	- 136	- 136	- 152	- 152
256 – 512	100	FM3	- 60	- 90	- 111	- 136	- 142	- 142	- 152	- 152
128 – 256	50	FM3	- 66	- 96	- 117	- 142	- 148	- 148	- 152	- 152
64 – 128	25	FM3	- 72	- 102	- 123	- 148	- 152	- 152	- 152	- 152
32 – 64	12.5	FM3	- 78	- 106	- 129	- 152	- 152	- 152	- 152	- 152
16 – 32	6.25	FM4	- 84	- 114	- 135	- 152	- 152	- 152	- 152	- 152
8 – 16	3.12	FM4	- 90	- 120	- 141	- 152	- 155	- 155	- 155	-
4 – 8	1.56	FM4	- 96	- 126	- 147	- 152	- 155	- 155	- 155	-
2 – 4	0.78	FM4	- 102	- 132	- 152	- 152	- 155	- 155	-	-

The DC/FM ranges FM2/3/4 are not always available. It depends on carrier frequency.

DC FM Range 2 - typical SSB phase noise in dBc/Hz

Frequency Range, MHz	Slope Hz/V	1 Hz	10 Hz	100 Hz	1 kHz	10 kHz	100 kHz	1 MHz	10 MHz
4340 – 4500	16000	- 18	- 48	- 78	- 112	- 118	- 118	- 136	- 156
2048 – 4340	8000	- 24	- 54	- 84	- 118	- 124	- 124	- 142	- 162
1024 – 2048	4000	- 30	- 66	- 96	- 124	- 130	- 130	- 148	- 152
512 – 1024	2000	- 36	- 66	- 96	- 130	- 136	- 136	- 152	- 152
256 – 512	1000	- 42	- 72	- 102	- 136	- 142	- 142	- 152	- 152
128 – 256	500	- 48	- 78	- 108	- 142	- 148	- 148	- 152	- 152
64 – 128	250	- 54	- 84	- 114	- 148	- 152	- 152	- 152	- 152
32 – 64	125	- 60	- 90	- 120	- 148	- 152	- 152	- 152	- 152
16 – 32	62.5	- 66	- 96	- 126	- 152	- 152	- 152	- 152	- 152
8 – 16	31.2	- 72	- 102	- 132	- 152	- 155	- 155	- 155	-
4 – 8	15.6	- 78	- 108	- 138	- 152	- 155	- 155	- 155	-
2 – 4	7.8	- 84	- 114	- 144	- 152	- 155	- 155	-	-

DC FM Range 3 - typical SSB phase noise in dBc/Hz

Frequency Range, MHz	Slope Hz/V	1 Hz	10 Hz	100 Hz	1 kHz	10 kHz	100 kHz	1 MHz	10 MHz
256 – 512	10000	- 36	- 66	- 96	- 121	- 138	- 142	- 152	- 152
128 – 256	5000	- 42	- 72	- 102	- 127	- 144	- 148	- 152	- 152
64 – 128	2500	- 48	- 78	- 108	- 133	- 152	- 152	- 152	- 152
32 – 64	1250	- 54	- 84	- 114	- 140	- 152	- 152	- 152	- 152
16 – 32	625	- 60	- 90	- 120	- 146	- 152	- 152	- 152	- 152
8 – 16	312	- 66	- 96	- 126	- 152	- 155	- 155	- 155	-
4 – 8	156	- 72	- 102	- 132	- 152	- 155	- 155	- 155	-
2 – 4	78	- 78	- 108	- 138	- 152	- 155	- 155	-	-

CW and DC FM Range 4 - typical SSB phase noise in dBc/Hz

Frequency Range, MHz	Slope Hz/V	1 Hz	10 Hz	100 Hz	1 kHz	10 kHz	100 kHz	1 MHz	10 MHz
16 – 32	6250	- 50	- 80	- 110	- 135	- 152	- 152	- 152	- 152
8 – 16	3120	- 56	- 86	- 116	- 141	- 155	- 155	- 155	-
4 – 8	1560	- 62	- 92	- 122	- 147	- 155	- 155	- 155	-
2 – 4	780	- 68	- 98	- 128	- 152	- 155	- 155	- 155	-

PN9100 Specifications

Frequency range	: 2.0 MHz to 4.5 GHz : 2.0 MHz to 9.0 GHz with PN9151 option : 2.0 MHz to 18 GHz with PN9151 + PN9152 options
Output level	: + 13 dBm ± 2 dB
Frequency resolution	: 1 Hz up to 1024 MHz : 2 Hz from 1024 to 2048 MHz : 4 Hz from 2048 to 4500 MHz : 8 Hz from 4.5 to 9.0 GHz : 16 Hz from 9.0 to 18 GHz
Harmonics	: - 20 dBc up to 512 MHz : - 10 dBc above 512 MHz
Sub-Harmonics	: - 90 dBc up to 1024 MHz : - 30 dBc above 1024 MHz
Non Harmonics (Excepted line spurs)	: - 80 dBc up to 1024 MHz Increases by 6 dB for each above range

FM Mode:

The DC FM oscillator is designed to bring the lowest contribution to the noise of the output signal. For FM range 1, used for clean stable sources, there is no contribution at all. For the other ranges, the closing noise increases with the selected FM deviation, specifically close-in the carrier.

FM deviation:

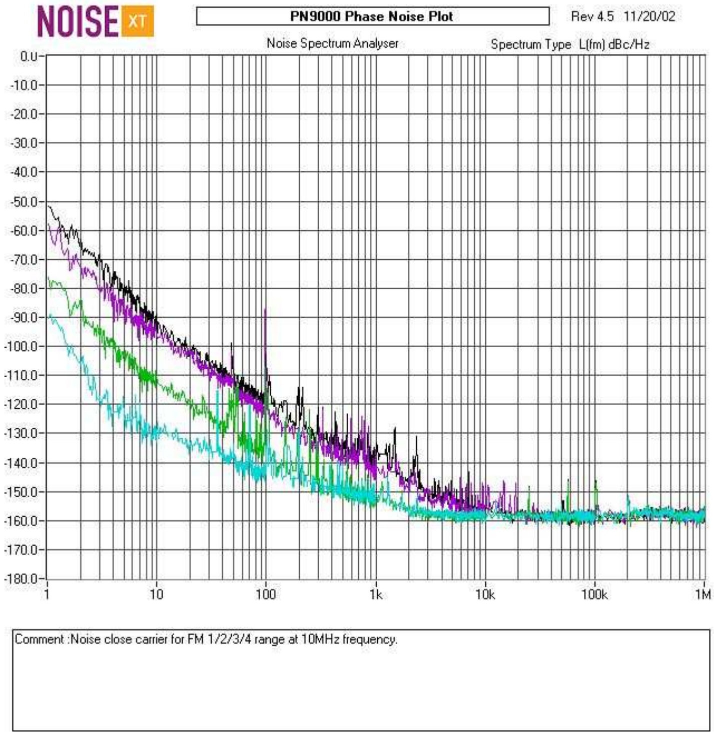
Four FM deviation ranges (FM1, FM2, FM3, and FM4) can be selected to comply with noise and phase/frequency fluctuation of the DUT. FM range 1 provides close residual noise as the CW mode, making the PN9100 the ideal reference source for any kind of stable source phase noise measurements.

Tables on page 7 show for each frequency range tune slope and SSB phase noise. Values are for 1 V peak. Input voltage range is ± 5 V, then for each frequency range full FM deviation is 10 times the slope/V. For Range 2 add 10 times more. FM deviation value is automatically set when selecting FM range and transferred to the loop parameters.

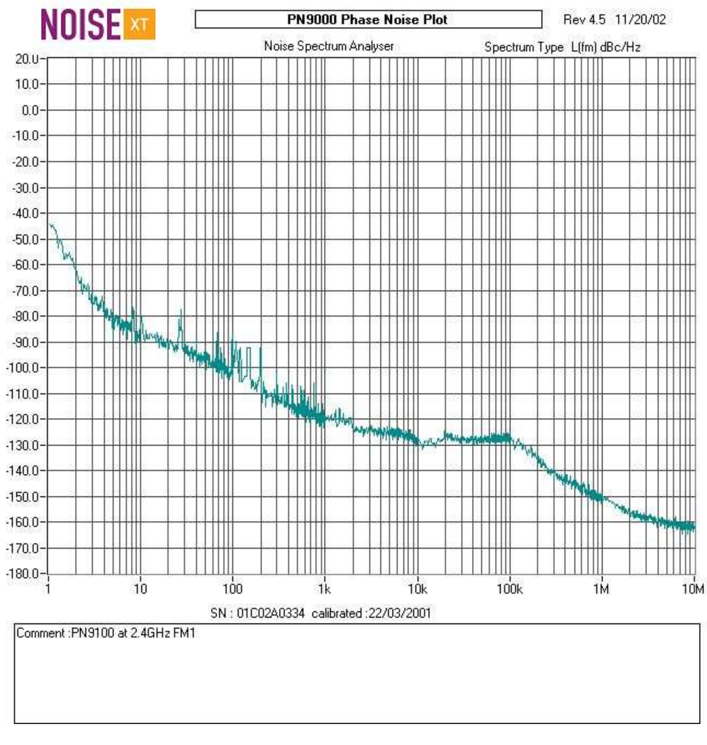
All figures are typical values, for specified values add + 3dB.

The PN9100 is made of three shielded modules housed in the back of the PN9000 mainframe, a PN9100 single slot output module located on the front of the PN9000 chassis and the PN9211 double size slot module reference time base.

When the configuration includes the PN9276 MW down-converter, the PN9211 is removed and replaced by the PN9276-4x, a shared time base.



Noise close to carrier depends on the FM range, example on a 10MHz carrier



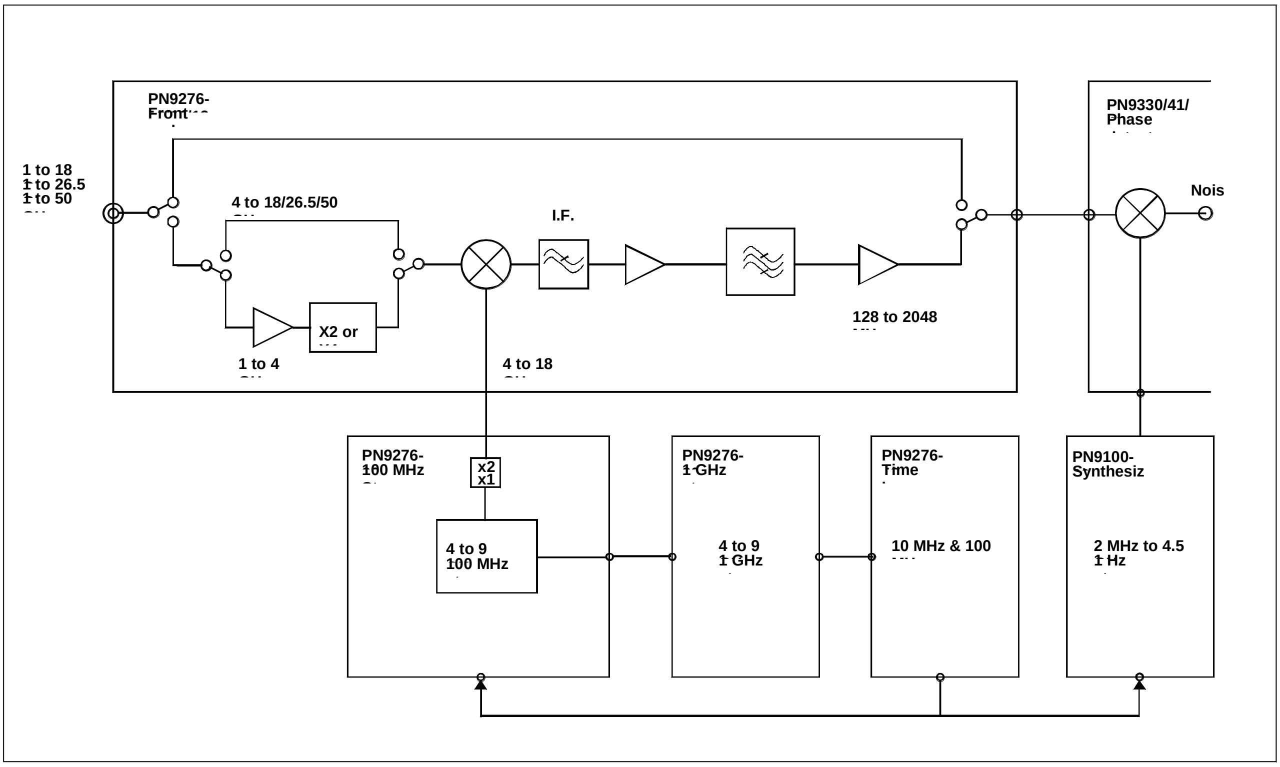
Example of a PN9100 measurement at a frequency of 2.4 GHz

PN9276
Microwave synthesized down-converter

The PN9276 down-converter includes a microwave down-converter stage driven by a low noise YIG based 100 MHz steps synthesizer. This synthesizer generates 4 to 18 GHz from a 100 MHz crystal oscillator phase locked onto a 10 MHz crystal oscillator, in order to provide low noise reference close-in and far away from the carrier.

This innovative architecture permits unprecedented performances.

Microwave down-converter operating diagram



The PN9276 generate 100 MHz steps and the PN9100 interpolates to work at any frequencies without loss of spectral purity.

PN9276 Specifications

Input Frequency range PN9276- 01 : 1 to 26.5 GHz
PN9276- 02 : 1 to 40 GHz

MW Signal Input Level : - 10 to + 0 dBm (add +10dB above 18GHz)

IF Output Frequency* :

	mode low IF	mode high IF
1 to 9 GHz	100 to 200 MHz	550 to 650MHz
9 to 18 GHz	100 to 300 MHz	550 to 750MHz
18 to 26.5 GHz	100 to 400 MHz	550 to 850MHz
26.5 to 40 GHz	100 to 700 MHz	550 to 1150MHz

*The IF frequency range depends on the span and the method of measurement, for wide span (> 40MHz) or Delay line method a higher IF is required.

IF output level -10 to 0 dBm for RF input up to 18GHz
-35 to -20 dBm above 18GHz RF input

Spurious response up to 18 GHz : <- 50 dBc from 1 Hz to 1 kHz offset
<- 80 dBc above 1 kHz offset

Down converter PN9276 Residual Phase Noise (dBc/Hz) :

For the phase noise specifications there is three modes: “Wide”, “Narrow” and “Standard” mode, corresponding to three locking bandwidths for the ouput mW Yig oscillator .

“wide” mode :
This mode is optimized for the lowest close-in noise up to 100 kHz from the carrier.

Frequency/Off set	1 Hz	10 Hz	100 Hz	1 KHz	10 KHz	100 KHz	1 MHz	10 MHz
1 GHz	-70	-98	-114	-138	-150	-151	-152	-168
2 GHz	-64	-92	-108	-132	-144	-145	-146	-168
4 GHz	-58	-86	-102	-126	-138	-139	-140	-162
8 GHz	-52	-80	-96	-120	-132	-133	-134	-160
16 GHz	-46	-74	-90	-114	-126	-127	-128	-154
20 GHz	-44	-72	-88	-112	-124	-125	-126	-152
26 GHz	-42	-70	-86	-110	-122	-123	-124	-150
40 GHz	-38	-66	-82	-106	-118	-119	-120	-146

“Narrow” mode:
This mode is optimized for the lowest noise far from the carrier (above 100 kHz).

Frequency/Off set	**1 Hz**	**10 Hz**	**100 Hz**	**1 KHz**	**10 KHz**	**100 KHz**	**1 MHz**	**10 MHz**
1 GHz	-70	-98	-106	-122	-136	-142	-162	-168
2 GHz	-64	-92	-100	-116	-130	-136	-156	-168
4 GHz	-58	-86	-94	-110	-124	-130	-150	-162
8 GHz	-52	-80	-88	-104	-118	-124	-144	-160
16 GHz	-46	-74	-82	-98	-112	-118	-138	-154
20 GHz	-44	-72	-80	-96	-110	-116	-136	-152
26 GHz	-42	-70	-78	-94	-108	-114	-134	-150
40 GHz	-38	-66	-74	-90	-104	-110	-130	-146

“Standard” mode:
This mode is the best compromise between the “Wide” and the “Narrow” mode .

Frequency/Off set	**1 Hz**	**10 Hz**	**100 Hz**	**1 KHz**	**10 KHz**	**100 KHz**	**1 MHz**	**10 MHz**
1 GHz	-70	-98	-112	-136	-146	-146	-158	-168
2 GHz	-64	-92	-106	-130	-140	-140	-152	-168
4 GHz	-58	-86	-100	-124	-134	-134	-146	-162
8 GHz	-52	-80	-94	-118	-128	-128	-140	-160
16 GHz	-46	-74	-88	-112	-122	-122	-134	-154
20 GHz	-44	-72	-86	-110	-120	-120	-132	-152
26 GHz	-42	-70	-84	-108	-118	-118	-130	-150
40 GHz	-38	-66	-80	-104	-114	-114	-126	-146

The figure shown is typical values, for specified values add + 4 dB. For frequencies above 18GHz, an external RF amplifier is required to adjust the level to the requirements of the Delay Line. Please add any thermal noise limits and noise figure due to the use of IF amplification if applicable.

Microwave Stable Source Down-converter (PLL measurement)

Configuration PN9276 (“Wide mode”) and PN9100 Residual Phase Noise (dBc/Hz) :

Frequency	Contribution	1 Hz	10 Hz	100 Hz	1 KHz	10 KHz	100 KHz	1 MHz	10 MHz
1 GHz	YIG down conv.	-70	-98	-114	-138	-150	-151	-152	-168
	9100	-78	-108	-129	-154	-160	-160	-164	-164
	Result	**-69**	**-98**	**-114**	**-138**	**-150**	**-150**	**-152**	**-162**
2 GHz	YIG down conv.	-64	-92	-108	-132	-144	-145	-146	-168
	9100	-72	-102	-123	-148	-154	-154	-158	-158
	Result	**-63**	**-92**	**-108**	**-132**	**-144**	**-144**	**-146**	**-157**
4 GHz	YIG down conv.	-58	-86	-102	-126	-138	-139	-140	-162
	9100	-66	-96	-117	-142	-148	-148	-152	-152
	Result	**-57**	**-86**	**-102**	**-126**	**-138**	**-138**	**-140**	**-151**
8 GHz	YIG down conv.	-52	-80	-96	-120	-132	-133	-134	-160
	9100	-66	-96	-117	-142	-148	-148	-152	-152
	Result	**-52**	**-80**	**-96**	**-120**	**-132**	**-133**	**-134**	**-151**
16 GHz	YIG down conv.	-46	-74	-90	-114	-126	-127	-128	-154
	9100	-60	-90	-111	-136	-142	-142	-152	-152
	Result	**-46**	**-74**	**-90**	**-114**	**-126**	**-127**	**-128**	**-150**
20 GHz	YIG down conv.	-44	-72	-88	-112	-124	-125	-126	-152
	9100	-54	-84	-105	-130	-135	-136	-152	-152
	Result	**-44**	**-72**	**-88**	**-112**	**-124**	**-125**	**-126**	**-149**
26 GHz	YIG down conv.	-42	-70	-86	-110	-122	-123	-124	-150
	9100	-54	-84	-105	-130	-135	-136	-152	-152
	Result	**-42**	**-70**	**-86**	**-110**	**-122**	**-123**	**-124**	**-148**
40 GHz	YIG down conv.	-38	-66	-82	-106	-118	-119	-120	-146
	9100	-48	-78	-99	-124	-130	-130	-148	-152
	Result	**-38**	**-66**	**-82**	**-106**	**-118**	**-119**	**-120**	**-145**

The figure shown is typical values, for specified values add + 4 dB. For frequencies above 18GHz, an external RF amplifier is required to adjust the level to the requirements of the Delay Line. Please add any thermal noise limits and noise figure due to the use of the phase detector RF and LO port gains if applicable.

Microwave unstable source Down-converter (Delay line measurement)

Configuration PN9276 (“Narrow” mode) and PN9718 :

Delay line 100 ns measurements : Residual noise (dBc/Hz)

Frequency	Contribution	1 KHz	10 KHz	100 KHz	1 MHz	5 MHz
1 GHz	YIG down conv.	-122	-136	-142	-162	-166
	Delay line 9718	-107	-137	-160	-170	-170
	Result	**-107**	**-133**	**-142**	**-161**	**-164**
2 GHz	YIG down conv.	-116	-130	-136	-156	-166
	Delay line 9718	-101	-131	-154	-170	-170
	Result	**-101**	**-127**	**-136**	**-156**	**-164**
4 GHz	YIG down conv.	-110	-124	-130	-150	-160
	Delay line 9718	-95	-125	-148	-168	-170
	Result	**-95**	**-121**	**-130**	**-150**	**-159**
8 GHz	YIG down conv.	-104	-118	-124	-144	-158
	Delay line 9718	-95	-125	-148	-168	-170
	Result	**-95**	**-117**	**-124**	**-144**	**-158**
16 GHz	YIG down conv.	-98	-112	-118	-138	-152
	Delay line 9718	-95	-125	-148	-168	-170
	Result	**-93**	**-112**	**-118**	**-138**	**-152**
20 GHz	YIG down conv.	-96	-110	-116	-136	-150
	Delay line 9718	-95	-125	-148	-168	-170
	Result	**-92**	**-110**	**-116**	**-136**	**-150**
26 GHz	YIG down conv.	-94	-108	-114	-134	-148
	Delay line 9718	-95	-125	-148	-168	-170
	Result	**-91**	**-108**	**-114**	-134	**-148**
40 GHz	YIG down conv.	-90	-104	-110	-130	-144
	Delay line 9718	-95	-125	-148	-168	-170
	Result	**-89**	**-104**	**-110**	**-130**	**-144**

The figure shown is typical values, for specified values add + 4 dB. For frequencies above 18GHz, an external RF amplifier is required to adjust the level to the requirements of the Delay Line. Please add any thermal noise limits and noise figure due to the use of external amplification if applicable.

Delay line 20 ns measurements : Residual noise (dBc/Hz)

Frequency	Contribution	1 KHz	10 KHz	100 KHz	1 MHz	5 MHz	10 MHz
1 GHz	YIG down conv.	-122	-136	-142	-162	-166	-168
	Delay line 9718	-94	-124	-147	-169	-170	-170
	Result	**-94**	**-124**	**-141**	**-161**	**-164**	**-166**
2 GHz	YIG down conv.	-116	-130	-136	-156	-166	-168
	Delay line 9718	-88	-118	-141	-163	-170	-170
	Result	**-88**	**-118**	**-135**	**-155**	**-164**	**-166**
4 GHz	YIG down conv.	-110	-124	-130	-150	-160	-162
	Delay line 9718	-82	-112	-135	-157	-167	-170
	Result	**-82**	**-112**	**-129**	**-149**	**-159**	**-161**
8 GHz	YIG down conv.	-104	-118	-124	-144	-158	-160
	Delay line 9718	-82	-112	-135	-157	-167	-170
	Result	**-82**	**-111**	**-123**	**-144**	**-157**	**-159**
16 GHz	YIG down conv.	-98	-112	-118	-138	-152	-154
	Delay line 9718	-82	-112	-135	-157	-167	-170
	Result	**-82**	**-109**	**-118**	**-138**	**-152**	**-154**
20 GHz	YIG down conv.	-96	-110	-116	-136	-150	-152
	Delay line 9718	-82	-112	-135	-157	-167	-170
	Result	**-82**	**-108**	**-116**	**-136**	**-150**	**-152**
26 GHz	YIG down conv.	-94	-108	-114	-134	-148	-150
	Delay line 9718	-82	-112	-135	-157	-167	-170
	Result	**-81**	**-106**	**-114**	**-134**	**-148**	**-150**
40 GHz	YIG down conv.	-90	-104	-110	-130	-144	-146
	Delay line 9718	-82	-112	-135	-157	-167	-170
	Result	**-81**	**-103**	**-110**	**-130**	**-144**	**-146**

The figure shown is typical values, for specified values add + 4 dB. For frequencies above 18GHz, an external RF amplifier is required to adjust the level to the requirements of the Delay Line. Please add any thermal noise limits and noise figure due to the use of external amplification if applicable.

Millimeter Wave Phase Noise Measurements

For devices above 50 GHz Noise XT quotes optimized solutions based on Harmonic Mixer down-conversion, up to 140 GHz (see mmW measurement pages further down).

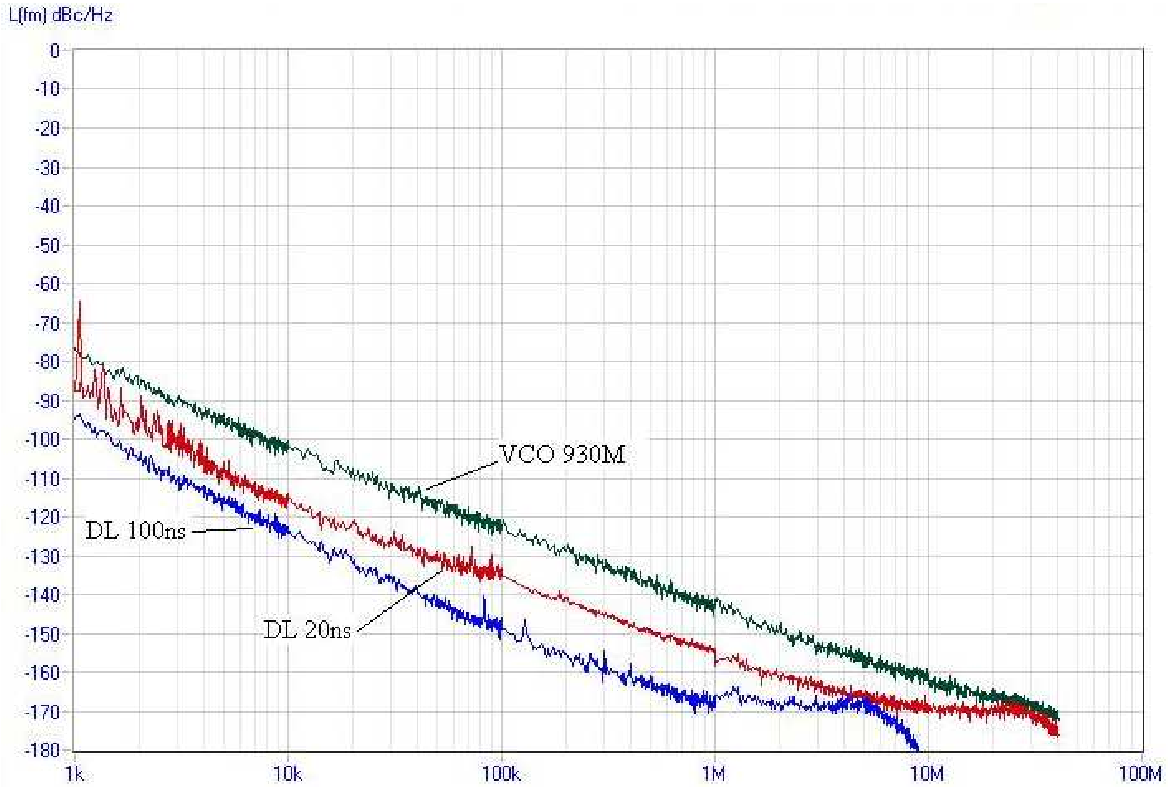
Two optional methods can be used to detect phase noise, reference phase locking or delay line. Delay line is the most convenient and the least expensive. As a matter of fact, the reference phase locking method requires two LOs, one from 5 to 9 GHz for the Harmonic Down-conversion, and the other, in the RF range, phase locked on the IF signal to detect phase noise. The delay line method needs the MW LO only, since the IF phase noise is detected by the delay line.

The optimized solution for mmW phase noise measurements includes a harmonic mixer, a diplexer-amplifier, the PN9100 built-in synthesizer with the PN9151 doubler option and PN9718 delay line. All options are housed in a PN9000 standard mainframe. Refer to mmW note/datasheet.

PN9000 DELAY LINES

For RF and MW Free-running Source Phase Noise Measurements

(From 250 MHz to 140 GHz)



To make easy measurements of the new generation of VCOs for mobile communications, Noise XT has designed this new delay line to provide higher phase noise detection sensitivity and lower noise floor up to :

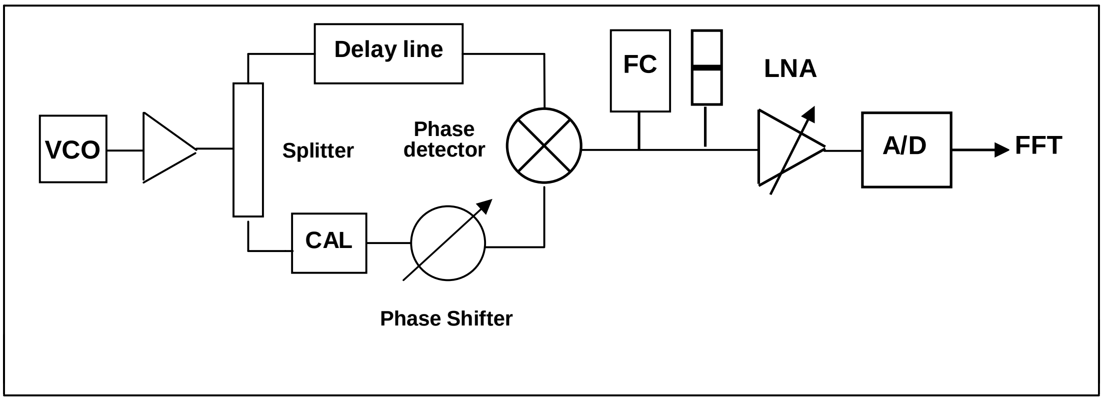
-130 dBc/Hz at 20KHz offset with the 100 ns .
-170 dBc/Hz at 20MHz offset with the 20 ns .

The above plot shows the residual noise, or noise floor, of the 20 and 100 ns delay lines measuring a 1 GHz very low noise SAW oscillator whose phase noise is lower. These plots include the phase noise of the 1GHz SAW oscillator itself (SAW noise floor : 168dBc/Hz at 2 MHz offset).

The upper plot shows a real 930 MHz GSM VCO. It shows that the residual noise is low enough to measure “state of the art” new generation VCOs.

PN9000 Delay Line Operating Diagram

The phase noise of Free-run frequency sources, such as VCO, DRO or YIG oscillators, cannot be easily measured using the reference phase locking method. Their frequency drift and phase/frequency fluctuations are generally too high to allow phase locking a DC FM reference source. Fortunately, another method can be used to obtain phase quadrature between RF and LO inputs of the RF phase detector of the PN9000 base system. Its principle of operation is shown below.



The DUT signal is connected to the power splitter through the input amplifier-conformer to compensate insertion loss of the delay line and the phase shifter. The power splitter outputs are connected to the RF input of the phase detector through the delay line and to the LO input through the calibrator and the phase shifter, which can adjust fine phase quadrature.
One button launches a complete measurement sequence.

The delay line operates as a frequency discriminator, since a delay line provides linear phase shift as a function of the frequency. When phase quadrature is achieved, the VCO's frequency fluctuations are converted into a noise voltage at the output of the phase detector. After spectrum analysis, the data is converted into the equivalent phase spectrum and displayed as a phase noise plot.

The demodulated signal, or noise voltage, is given by the following formula:

$$\text{Vnoise}\,(f_m) = K_\Phi\, 2\pi\tau\, \Delta f(f_m)\, [\sin(\pi\tau\, f_m) / (\pi\tau\, f_m)]$$

K_Φ is the sensitivity of the the phase detector, expressed in Volt/radian. The term sin(x)/x provides first null response of a delay line at $1/\tau$ offset, then the appropriate delay must be selected depending on the desired offset analysis, taking into account the residual noise depending on length of the delay line (see table below) The PN9000 software compensates for the sin(x)/x response to provide accurate measurements up to 5MHz for 100 ns delay, 30 MHz for 20 ns.

Note: Unlike the reference phase locking method, the delay line provides poor AM noise rejection. As a consequence, when AM noise is significant compared to phase noise, the measurement result will show a combination of both. This is why the delay line method is dedicated for free running oscillators with no or low AM noise.

Operating frequency range is 250 MHz to 2 GHz. A family of VCO Up/Down converters extends the frequency range from 2 GHz to 26.5 or 40 GHz. From 40GHz to 140GHz, Harmonic mixers driven by the MW LO source down-convert mmW free-run sources to the operating range of the delay lines. (see mmW note)

PN9281 with PN9293-xx

mmW PHASE NOISE MEASUREMENT

Down-conversion to the RF frequency range

As for the MW sources, the mmW sources must be down-converted to the operating range of the PN9000 system. The most convenient way to do this is to use a Harmonic Mixer. These devices are designed to work with LO harmonic ranks as high as 11 to 13, providing an IF signal of - 30 dBm or higher so that it is possible to down convert a mmW signal of 20 to 140 GHz with an LO source of 4 to 9 GHz.

Phase Noise Detection Methods

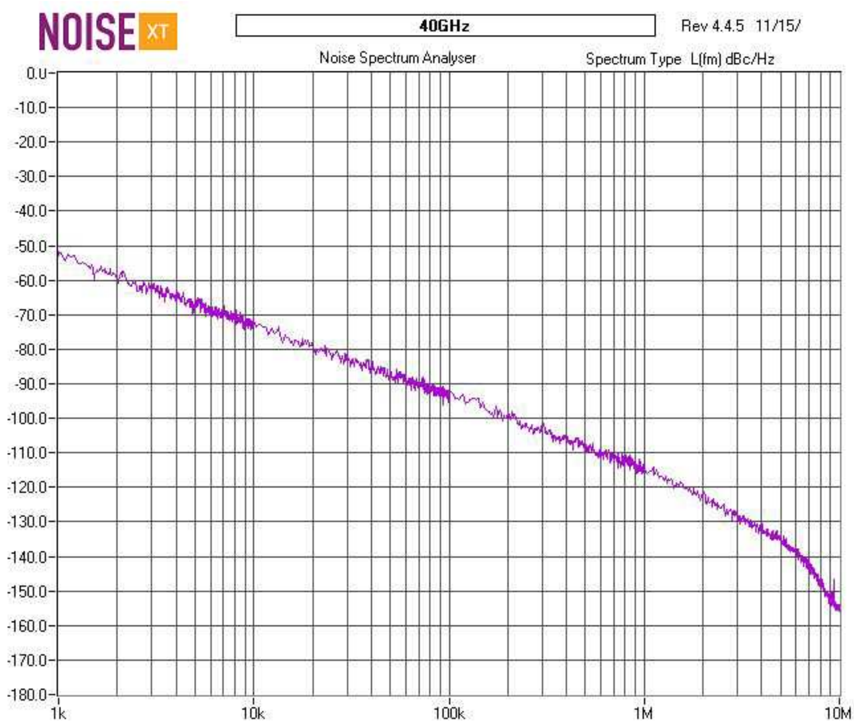
When converted to the RF range the phase noise of the DUT signal can be detected by the mean of two methods: the Reference phase locking method or Delay line method.

The Reference Phase Locking method will be used, as for the RF and MW devices, for clean phase locked mmW sources. As shown below, it requires a MW LO in the range of 4 to 9 GHz depending on the mmW signal frequency and an RF reference synthesizer up to 2 GHz.

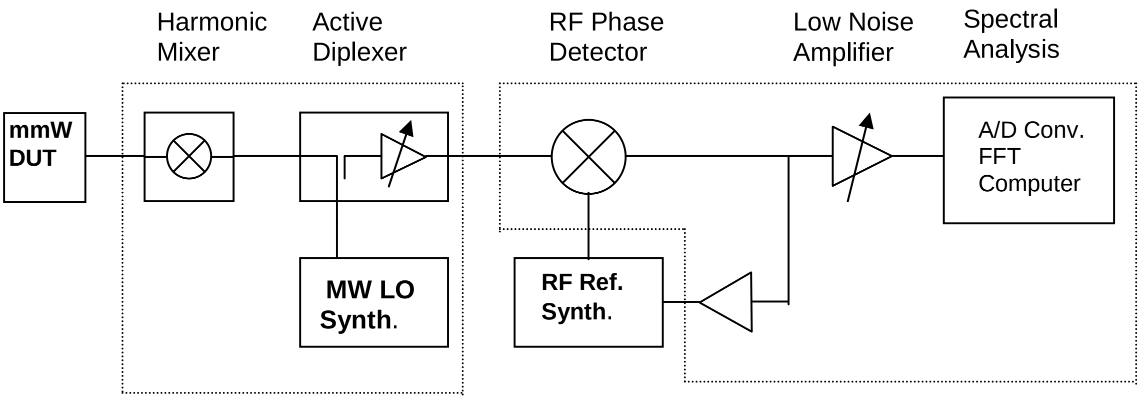
The Delay Line Method will be used for the noisy phase locked and free running sources.
However, it appears that the residual noise of the PN9000 delay lines is lower than that of most of the phase locked mmW sources, so that they can be measured using the delay line method.

The Delay Line method offers two main advantages:

Only one LO synthesizer is required for the mmW down conversion.
The PN9000 delay lines include automatic process for phase quadrature adjust and calibration.

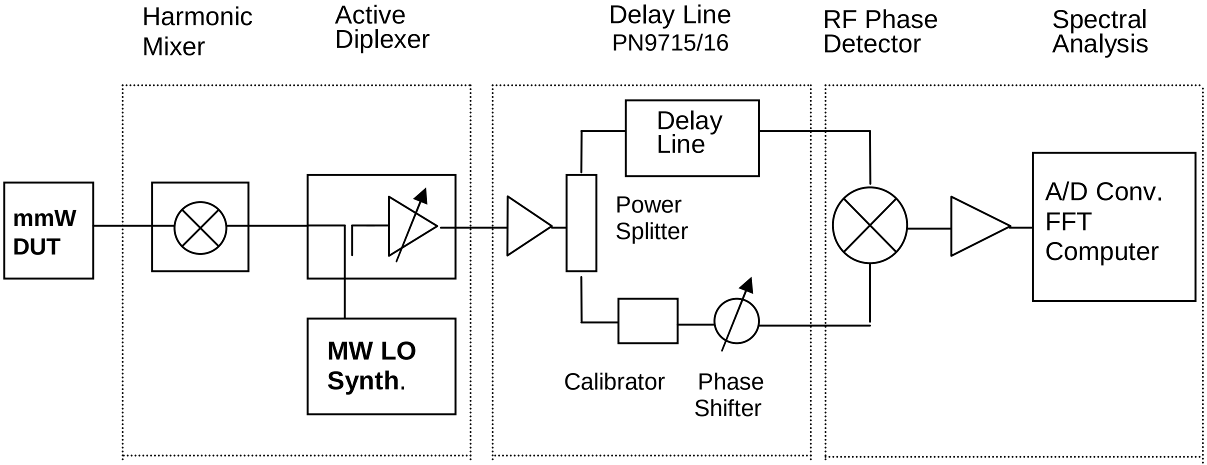


Reference Phase Locking Method



The mmW harmonic mixer is selected according to the DUT frequency. As a general rule they cover an octave. PN9000 options cover 40 to 140 GHz. At first measurement it is recommended to connect a spectrum analyzer to the output of the diplexer and tune the LO synthesizer to optimize the IF level and frequency, and adjust the gain to get between 0 and + 10 dBm at the input of the RF phase detector. Then the major steps to make a measurement are: tune the RF Reference synthesizer to IF value from the diplexer, measure the beat at the output of the phase detector, calibrate the phase detector, execute phase lock, and measure. The RF Reference synthesizer can be the PN9100 or any appropriate external signal generator.

Delay Line Method



Use the same procedure as above to optimize IF Level and Frequency. Then, just run the delay-line automatic measurement process. This method allows easy and fast measurements.

Note: The PN9000 harmonic mixer options cover the following ranges: 33-50, 40-60, 75-110, 90-140, 50-75, 60-90 and 90-140 GHz. When existing harmonic mixers include a diplexer, the PN9281 diplexer is removed. However the PN9281 controlled amplifier is recommended to adjust the IF output level at the operating amplitude range of the phase detector.

PN9820

BUFFER - AMPLIFIER - ISOLATOR

Most of the problems which occur when performing phase noise measurements come from:

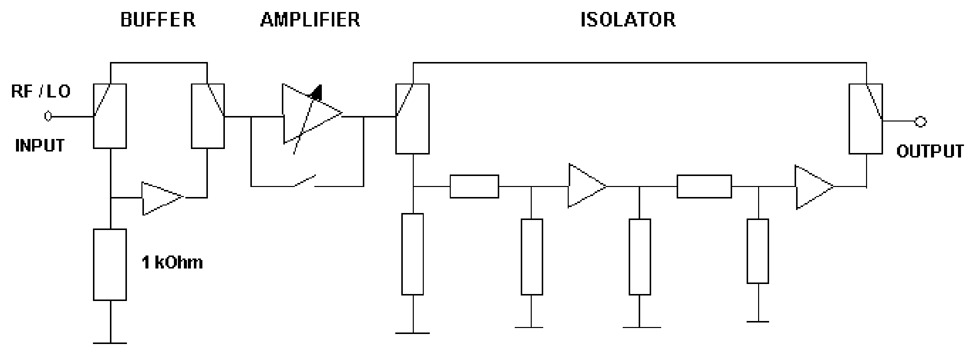
- Low DUT output level,
- High DUT output impedance (TTL output), connected to 50 Ohm PN9000 RF input,
- Poor isolation between the oscillator and the output of the DUT, which is at the origin of DUT locking injection from the Reference source through the RF and LO inputs of the phase detectors.

The solutions consist in providing input gain, impedance adaptation and isolation between the RF and LO inputs of the phase noise detector. That is what the Noise XT PN9820 option provides. It is housed in a standard PN9000 double slot module. The three functions and parameters are controlled from the PN9000 software. Thus, it is possible to select the appropriate functions depending of the DUT source parameters.

The PN9820 is a dual channel Buffer - Amplifier - Isolator, with full software control. One channel is for the DUT source and the other one is for the LO source. They have separate software control.

PN9820 Specifications

Frequency Range		: 5 MHz to 1.8 GHz	
Amplifier Nominal Gain		: F < 1 GHz	: 0 - 10 - 20 - 30 dB
		F > 1 GHz	: 0 - 7 - 14 - 21 dB
Insertion loss		: F < 100 MHz	: 1.3 dB
		F < 1 GHz	: 3 dB
		F> 1GHz	: 7 dB
Noise factor		: amplifier only	: 5 dB
		Isolator only	: 15 dB
Buffer	: 1 kOhms	: F < 100 MHz, gain = 7 dB	
	100 Ohms	: F < 1 GHz, gain = 0 dB	
Isolator		: F < 100 MHz, 50 dB	
		1 GHz, 70 dB	



Note: One channel only is represented

Switches controlled by the software allow selection of the desired functions and adjust the gain of the amplifier to provide the optimized output levels for the RF and LO inputs of the phase detectors (0 to +10 dBm for the RF input and +6 to +10 dBm to the LO input.)

PN9908
FREQUENCY DOUBLER ISOLATOR

This option has been designed for two purposes. The first is to prevent injection between the reference source and the DUT through the phase detector; the second is to increase the system measurement dynamic range.

Isolation against Injection locking, between Reference and DUT sources in PLL mode

Due to low isolation between the RF and LO input of the phase detector, the DUT and Reference can synchronize on each other when they are tuned on the same frequency instead of phase locking the reference on the DUT. Without phase locking, there is no phase quadrature and no phase noise detection. This problem happens often with small TTL or ECL devices having high output impedance. This phenomenon is known as “injection locking”.

There are two solutions to provide isolation between the DUT and reference.

> The first is to insert attenuators between the DUT output and RF input and the Reference output and LO input. However, if more than 10 dB are needed, the RF and LO input levels will be too low. Then amplifiers will have to be inserted between the attenuators. Noise XT has designed such an option, the PN9820 Amplifier Isolator.
>
> The second solution is to double the DUT and Reference signals. In this case, the DUT and Reference sources do not see their fundamental frequency through RF/LO leakage of the phase detector. The PN9908 provides in consequence a virtual (but real) isolation between the DUT and Reference sources.

Increase the System Dynamic Range using the Delay line Mehtod

For exmple, if the system residual noise is - 160 dBc/Hz at 1 MHz offset and the expected noise of the DUT is – 163 dBc/Hz. The system will of course measure – 160 dBc/Hz and not the actual noise of the DUT.
The PN9908 will double the DUT signal frequency and, its phase noise will increase by 6 dB (20LogN) to – 157 dBc/Hz, i.e. 3 dB above the delay line residual noise. The software includes a function to deduct the 6 dB added to the measured values. The PN9000 has a reference offset function to do this automatically.

Specifications PN9908

Frequency range	: 100 MHz to 1 GHz, 1 GHz to 2.2 GHz (2 bands selectable by software)
Input level	: -5 to + 5 dBm / 50 Ohm.
Function	: Low noise Frequency Doubler
Size	: 1 single PN9000 slot module

PN95XX

Reference Crystal Oscillators

All stable frequency sources, such as synthesizers used in radar, satellites, digital and mobile communication systems, utilize reference crystal oscillators. Their phase noise, often very low, must be measured to make sure it doesn't affect the performances of the whole system they drive. However, it is often difficult to find another reference good enough to measure them. Noise XT offers a selection of very low and ultra low noise reference crystal oscillators housed in standard PN9000 modules, making the measurements easy and accurate.
In addition to the following standard catalog devices, Noise XT will quote on request customized frequencies.

Parameters	**PN9510** **Very low noise**	**PN9511** **Ultra low noise**	**PN9530** **Very low noise**	**PN9531** **Ultra low noise**
Frequency	10 MHz	10 MHz	100 MHz	100 MHz
Output level, typical	+ 10 dBm	+ 13 dBm	+ 10 dBm	+ 13 dBm
Long term stability	5.10^{-10} / day after 3 months operating	NA	NA	1.10^{-9} / day after 1 month operating
Frequency tuning				
- Mechanical	NA	2 ppm	NA	± 2.5 ppm
- Electrical	2 ppm	2 ppm	10 ppm	± 0.2 ppm
- Tune voltage	0 to + 10 V.	0 to + 10 V.	0 to + 10 V	± 5 V
- Average tune slope	2 Hz / Volt	2 Hz / Volt	150 Hz / V	4 Hz / V
Phase noise, dBc/Hz				
10 Hz	- 132	- 134	- 95	- 100
100 Hz	- 142	- 162	- 125	- 130
1 kHz	- 148	- 172	- 155	- 162
10 kHz	- 152	- 174	- 168	- 178
100 kHz	- 152	- 174	- 168	- 178
1 MHz	- 152	- 174	- 168	- 178

- All phase noise figures are typical values, add + 5 dB for specified values
- Other frequencies are available, such as 10.23, 13, 26, 70, 140 MHz. Request for quotation.
- All are housed in standard single size PN9000 modules

PN9562

REFERENCE SAW OSCILLATOR 1GHz

This oscillator provides, due to the SAW resonator, a very low phase noise signal. Running at 1 GHz, its phase noise is at the order of magnitude of that a 100 MHz crystal oscillator. It provides much better phase noise than a 100 MHz crystal oscillator multiplied 10 times.

Such a low noise 1 GHz source has a lot of applications. It can be used as a reference for MW PLLs and converters. It can also be used as a reference for phase noise measurements. As a matter of fact, it is one of the best 1 GHz frequency source available today.

PN9562 Specifications

Frequency	: 1 GHz	
Tune Range	: ± 300 KHz	
Tune Voltage	: 0 to + 5 V	
Output Power	: + 10 dBm typical, + 7 dBm min.	
Output Impedance	: 50 Ω	
Phase Noise, in dBc/Hz	: - 80	at 100 Hz offset
	- 112	1 KHz
	- 135	10 kHz
	- 160	100 kHz
	- 168	1 MHz
	- 168	10 MHz
Size	: single PN9000 slot	
Operating temperature	: 0 to + 50°C.	

All phase noise figures are typical values, add + 5 dB for specified values

PN9815

Pulse Generator and Modulator

Low noise Pulsed CW in PLL and and Added Noise measurements require a low jitter pulse generator and high ON/OFF pulse modulators (MW switches).

The PN9815-00 (master) includes :

- A crystal oscillator clock, for low noise jitter
- A Pulse generator, to generate the trigger and the pulse waveform
- A MW Pulse modulator to switch on/off the microwave carrier

The PN9815-01 (slave) is used to generate a second pulse modulator. Some measurements require the same pulsed CW signal on the RF and LO phase detector inputs.

The PN9815-01 slave uses the same clock as the PN9815-00 master. An internal connection in the PN9000 mainframe provides the clock to PN9815-01. In case this option is supplied as a later add-on, a mainframe modification is necessary.
This microwave pulser can be connected to the output of the PN9100 or PN9276 to generate a pulsed CW source.
The pulse generator output (TTL 50 Ohms) can be used to switch on/off an external DUT.

The "trigger out" can be used to trigger the external DUT.
The "trigger in" can be used to trigger the PN9000 microwave pulse modulator from an external system.
If the two sources are pulsed (the reference source and the DUT), the two pulses must be synchronized.

PN9815 Specifications

Clock, internal	:20 and 200 ns
Trigger	:Internal or external
Trigger output	:TTL positive/50 Ohm. Duration : 20 or 200 ns
Cycle/PRF	:Min : 40 or 400 ns (2.5 MHz or 25 KHz) Max : 20 ns x 65536 = 1.3 ms or 200 ns x 65356 = 13 ms
Pulse width	: Min : 20 or 200 ns
Pulse out	: TTL positive/50 Ohm
Pulse RF output	: Same level as the input signal, must be loaded on 50 Ohm. During OFF time, the RF signal is internally loaded on 50 Ohm. The pulse signal is internally connected to the SPDT.
Delay 1 to 2	: Delays the master trigger for the PN9815 slave, to adjust the output pulse according to delays in the DUT and connectors.
Min delay	: 0
Max delay	: 20 or 200 ns x 256

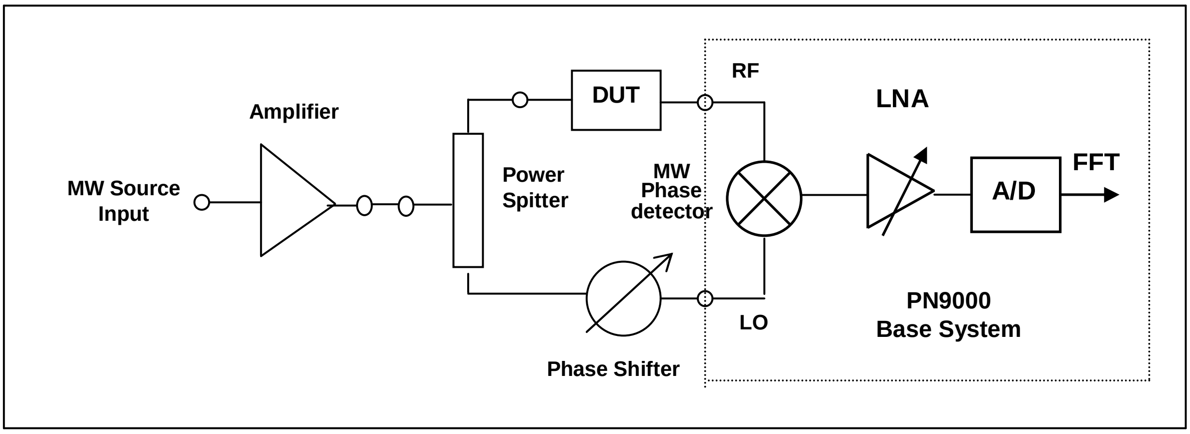
PN9841

For Added Phase Noise Measurements

The PN9841 option includes, in a two-slot module:

An amplifier, connected when the input level is too low.
A power splitter to split the input signal in two paths, one to the RF phase detector input through the DUT and the other to the LO phase detector input through the phase shifter.
An external phase shifter, also called motorized trombone.

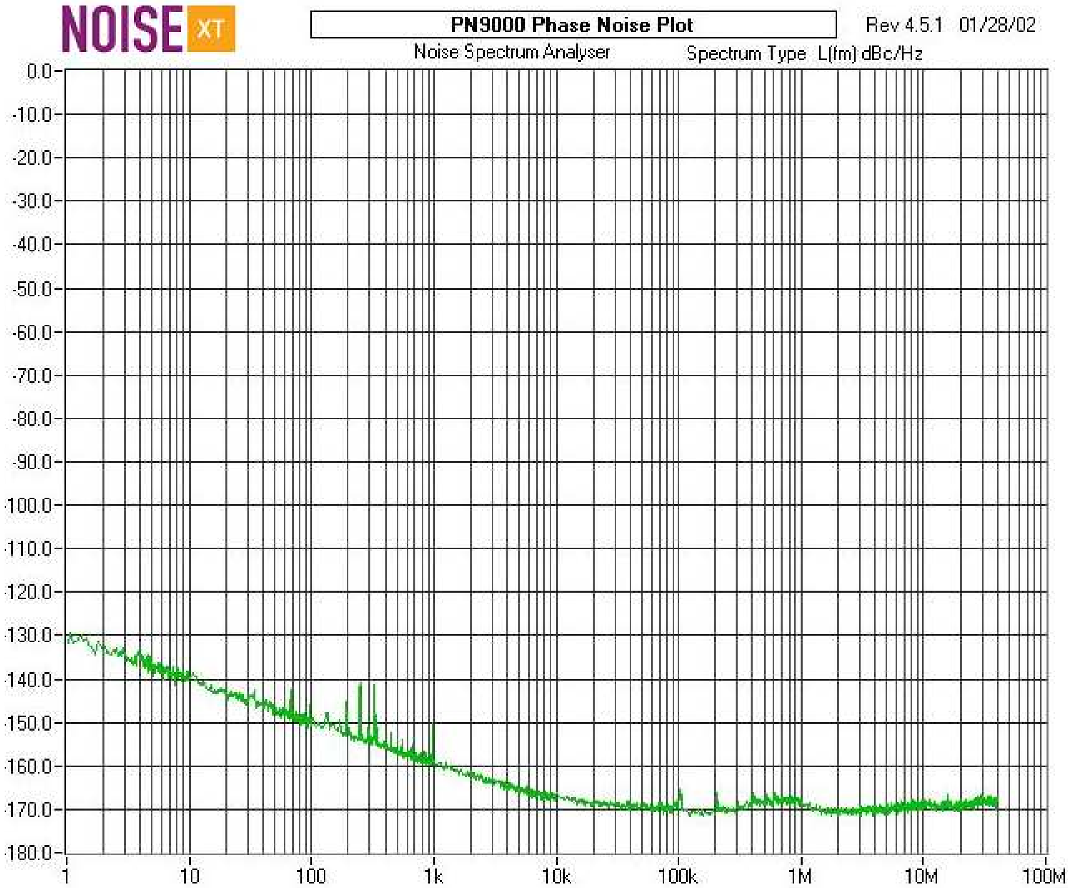
The other components, MW phase detector, FC, bar graph, LNA, etc. are part of the base system.



PN9841 Specifications

Frequency range	: 2 to 18 GHz depending on phase shifter
Input amplifier level	: 0 dBm min. for maximum measurement dynamic range
Input amplifier gain	: 15 / 20 dB
Phase shifter output level to LO	: +7 dBm min
Output level to DUT input	: + 12 to +15 dBm

The output level of the DUT should be adjusted to the nominal value of the RF input port (0/+6 dBm for phase adjust calibration mode and up to the maximum power input).



Residual Added Noise Measurement at 10 GHz

For principle of operation, see "ADDED PHASE NOISE MEAUREMENT" application note. Where do I find these as a customer? see page 39

For measurement process, see "PULSE CW MEASUREMENTS" technical note.

For Pulse modulation option, see PN9815 datasheet.

Added phase noise residual specification:

10 Hz	100 Hz	1 kHz	10 kHz	100 kHz	1 MHz	10 MHz
- 130	- 135	- 140	- 155	- 160	- 160	- 160

PN9000

Phase Noise Measurement System

Application and Information

Measurements in MW Frequency range

When the DUT signal frequency exceeds the operating frequency range of the PN9000 base system, 1.8 to 2 GHz, the measurement solution will depend on the nature of the DUT stable or free running source. Stable sources are PLL or synthesizers. Free running sources are those with no phase locking on a reference crystal oscillator.

For the stable sources, the PN9000 offers two solutions:

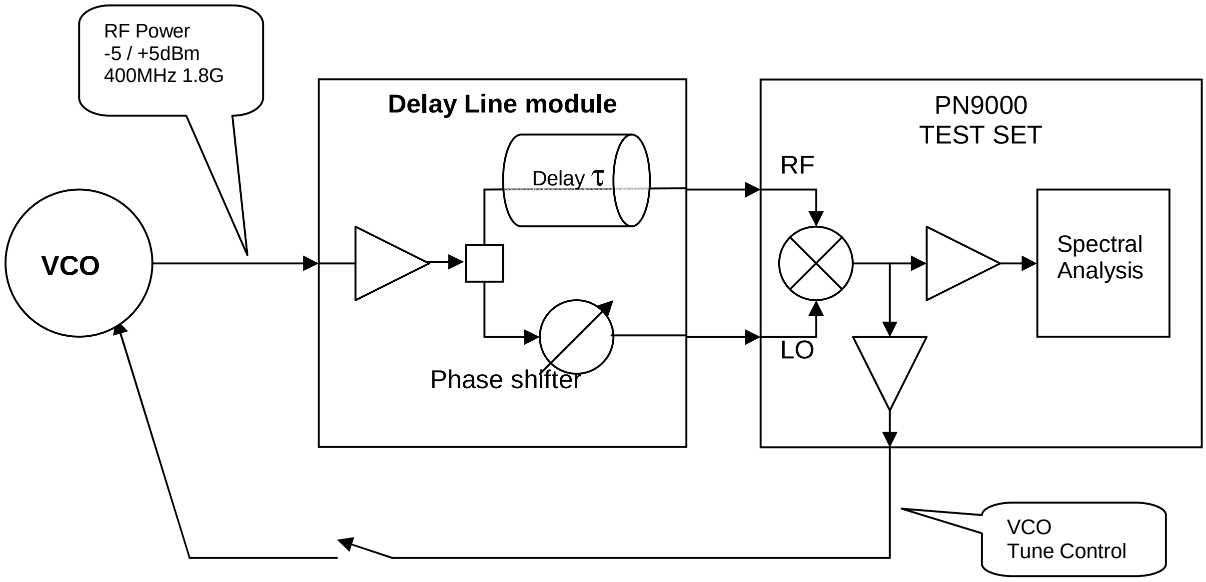
The PN9273 & PN9274, 18 & 26.5 GHz down-converters
They include low noise oscillators and a MW mixer to provide an IF signal connected to the RF input of the PN9000 base system. The phase noise is detected using the PN9100 as the LO reference.
This solution provides the lowest residual noise, due to the low noise fixed frequencies used to down convert the DUT to the RF frequency range and the low noise of the PN9100.

The direct phase noise detection up to 4.5, 9.0, 18 & 26.5 GHz
The standard PN9330 RF phase detector is replaced by the PN9341 MW phase detector. To the PN9100 RF reference synthesizer will be added the PN9151, 4.5 – 9.0 GHz and the PN9152, 9.0 – 18.0 GHz doublers. Each one increases the phase noise by two times or 6 dB, i.e. 12 dB between 4.5 and 18 GHz. For the range from 18 to 26.5 or 40 GHz (PN9361), the MW phase detector works on the third harmonic of the LO.

For Unstable or Free Running Sources

These sources are not phase locked. Their short and long term stability depend on their frequency range, component quality and technology. In general, their drift and frequency fluctuations are too high to phase lock a reference, the delay line method is the only way to detect their phase noise. (See Delay line method in the PN9000 description and Delay line datasheet.)
The maximum direct input frequency range of the delay lines is 2.0 GHz. Then, to measure free running sources at a higher frequency, the MW DUT signal must be down converted to the operating range of the delay lines.
Phase locked MW sources such as the PN9276 MW down-converter and PN9100 + PN9151/52 can be used, however, the noise floor of a free running oscillator is generally lower than that of a phase locked oscillator due to the noise of the loop components, digital divider, amplifier and varactor. This is why, to measure the phase noise of a MW free run source, the LO used to down convert it must also be a free run source.
The PN9276 is capable of changing its phase lock loops to behave as a free running oscillator and provide the best phase noise.

VCO Measurements



The Delay line method acts as a frequency discriminator. Since a delay is a linear phase shift with frequency, the frequency fluctuations of the VCO are converted into a noise voltage at the output of the phase detector. After the spectral analysis has been performed, the system transforms the frequency spectrum into the equivalent phase spectrum and displays the curve in the same format as with the direct phase demodulation method. The conversion is inversely proportional to the offset frequency squared, $1/f^2$. Due to this conversion, the residual white noise of the test set is transformed into a $1/f^2$ noise. The sensitivity of this demodulation decreases by 20 dB per decade as the offset frequency of measurement decreases (see curve).

This method is very useful for measuring sources that have a high amount of frequency drift, such as free running VCO. A 100 nsec delay line allows 250 KHz frequency drift without affecting the measurement accuracy. It also enables the measurement of a source without a lower noise reference source, but if the residual noise shape of the delay line method is adapted to a VCO phase noise spectrum, it is not an adequate method for synthesized sources which present lower close in phase noise.

The demodulation is proportional to the length of the Delay Line (τ):

$$\text{Noise Voltage } (f_m) = K_\Phi \, 2\pi\tau \, \Delta f (f_m) \, [\sin(\pi\tau f_m) / (\pi\tau f_m)]$$

K_Φ = phase detector demodulation factor

$\Delta f (f_m)$ = frequency fluctuations of the VCO, function of the offset.

The PN9000 software corrects the [$\sin(\pi\tau f_m) / (\pi\tau f_m)$] transfer function up to about $f_m = 1/2\tau$

$$\text{Noise Voltage } (f_m) = K_\Phi \, 2\pi\tau \, \Delta f (f_m) \quad \text{up to } f_m = 1/2\tau .$$

The compromise of this method is between the sensitivity proportional to τ and the maximum offset frequency of the measurement inversely proportional to τ. The PN9000 system proposes different values for the delay line:

- 100nsec: sensitivity –148dBc/Hz at 100KHz offset, Foffset max = 5MHz, VCO drift 250KHz
- 20nsec: sensitivity –135dBc/Hz at 100KHz offset, Foffset max = 25MHz, VCO drift 1.25MHz
- 20nsec: sensitivity –170dBc/Hz at 20MHz offset.

Measurement Process

The VCO is connected to the Delay Line module input and the signal is amplified to +20 dBm with a limiting power amplifier.
The phase detector demodulation factor expressed in Volts per radian has to be measured to refer the spectral density of the phase noise to 0dBc/Hz, which represents the carrier power or 1radian rms of phase jitter.

In case of a two-source configuration, a beat note frequency is set between the two paths RF and LO. The system then measures the phase slope at 0Volt crossing, corresponding to the quadrature condition. For the Delay Line configuration with only one source, one of the easiest solutions is to adjust the two paths in quadrature and move the phase between the two paths, RF and LO, by a calibrated amount $\Delta\Phi$ and measure the DC voltage ΔV at the output of the phase detector:

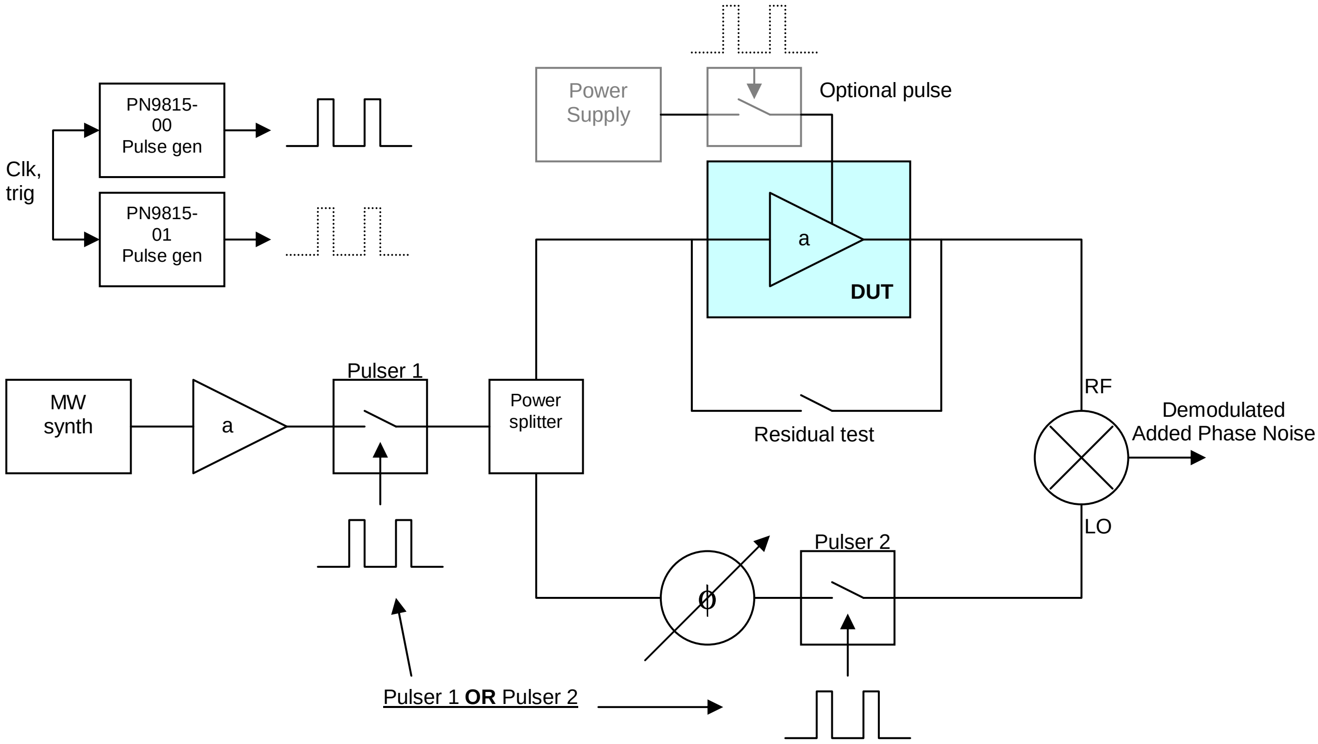
Demodulation factor $K_{\Phi} = \Delta V / \Delta\Phi = \Delta V / 2\pi F_o \Delta\tau$
With F_o the VCO carrier frequency.
F_o is measured with the internal RF frequency counter.

The electronic phase shifter operates automatically this quadrature adjustment and measurement.
The losses of the Delay Line are proportional to the carrier frequency. Above 1GHz the sensitivity decreases by 20 log (1GHz / F_o GHz).

In case of large frequency drift, the VCO can be locked by the Voltage Control to maintain the quadrature condition without affecting the spectrum above 100Hz offset.

ADDED PHASE NOISE

Measurement for two-port devices



Depending on the measuring configuration, pulse modulator 1 or 2 are used. When no signal is connected to their input, they are ON (CW mode).

This method quantifies the amount of noise added to a signal as it passes through a DUT.
The technique of measurement is the same as the Residual Test of the phase detector method, determining the noise floor of a system.
A Residual Test (DUT bypassed) is performed by dividing the source output with a power splitter "Sp" and phase shifting one path "Ps" by 90°. The two signal paths RF and LO enter the mixer in quadrature with correlated phase fluctuations. The measured noise is only generated by the test set itself as long as the delay difference of the signal paths is minimized to reject the Source frequency (or phase) noise.
In case of Added Noise measurement, the DUT is inserted in the RF path so that the measured noise is the sum of the residual noise (DUT bypassed) and the added noise of the DUT.
This measurement can be performed under CW or Pulsed conditions.

The different parts of the setup are:

Source (microwave synthesizer)

The Source is at the test frequency. Its absolute phase noise is reduced by the correlation factor given by 20log ($2 \pi \tau Fm$).
With τ = delay difference of the two paths, Fm = frequency offset

Example: absolute phase noise of the Source = -50dBc/Hz at 100Hz from the carrier, τ = 10ns and Fm = 100Hz, correlation factor = -104dB, the noise floor only due to the Source is -50dBc/Hz -104dB = -154dBc/Hz at 100Hz from the carrier.
Another caution is the AM noise of the Source, the phase detector has approximately only 30dB AM rejection. AM contribution can be estimated by setting the two paths in phase. In this condition the mixer demodulates the AM noise. From this noise only 30dB reduction can be achieved when the two paths are in quadrature.

Power Amplifier "A" (+20dBm)

To achieve a good dynamic, the PN9000 has a high level phase detector requiring LO power > +15dBm and RF power > +10dBm which correspond to approximately +20dBm before the power splitter. A power amplifier is needed because the majority of the microwave sources don't provide +20dBm output power.

Pulser "Pu"

If the DUT is operating under pulsed conditions it is better to provide pulsed signal on the two paths. This way the DC offset and the internal phase noise of the phase detector are minimized.

Isolator "Is"

An isolator can be inserted in the RF path to prevent bad SWR at the input of the DUT.

Phase shifter "Ps"

The phase shifter can be mechanical or electrically tunable. This phase shifter is used for two purposes: to adjust the phase to measure the demodulation factor and to adjust the phase to set the quadrature. An electrical phase shifter presents two limitations: its internal added noise can be too large and the maximum input power can be too low to be compatible with the high-level phase detector
The PN9000 provides three main advantages when testing Added Phase Noise under pulsed conditions:

A PRF video filter can be inserted between the phase detector and the low noise amplifiers.
The low noise amplifiers support a large voltage swing.
The High Level mixer provides a high demodulation factor.

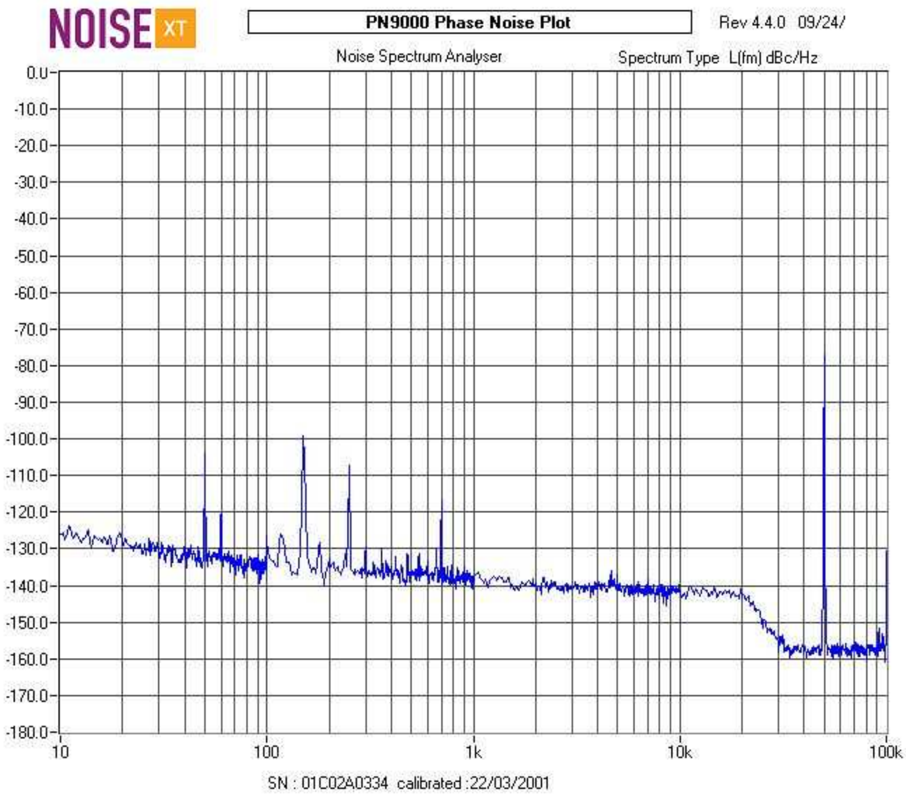
These features permit the best dynamic under pulsed conditions.
The process of measurement is the same as CW, except that in the calibration process the video filter has to be selected. The system takes into account the loss of sensitivity due to the Duty Cycle and the spectrum is then normalized.

Hardware Configuration

The PN9000 family offers an "ADDED NOISE" option including:
A Power Amplifier, a Pulser, a Power Splitter, a Phase Shifter, a Pulse generator with low jitter and video filters. The pulse generator includes an external trigger and auxiliary output to drive the DUT with a programmable delay 20ns to 1ms between the microwave pulse and the DUT pulse.

The PN9100 Low noise synthesizer is the adequate Source providing the lowest phase and amplitude (AM) noise.
The phase noise test set PN9000, the Added noise module and the PN9100 are housed into a standard 3U chassis, offering a compact system including all the hardware to perform Added noise measurements.

Pulsed CW Source phase noise



This plot shows the measurement of a 3.5 GHz signal modulated by the PN9815. PRF is 50 KHz and the duty cycle is 5%.

For measuring a pulse CW modulated signal the PN9000 must cope with the following problems:

Loss of power

The average, or rms power, decreases as a function of the duty cycle of the pulse signal. The exact same process happens to the demodulation factor. Its variation is given by the formula 20 log (duty cycle). Thus, for 10 % duty cycle the demodulation factor (and noise floor) is 20 dB lower (higher) than it is in CW, and for 1% duty cycle it is 40 dB difference (add +40dB to a CW residual noise floor !). To display the real noise of the modulated signal the software will have to compensate by computing an offset corresponding to the duty cycle. This is why the software menu needs the duty cycle value (or also called “pulse ratio”)
In general this is not a problem because pulsed sources are mostly in MW range and have higher phase noise than RF sources. However, attention must be paid to it.

The system also has to compensate for the loss of phase lock loop sensitivity due to the duty cycle.

With lower input power, calibration of the phase detector could be tricky. To prevent that, the PN9000 software includes additional gain adjustment, used only for calibration.

Bessel response spurs

The power of a pulsed signal is split around the carrier on the fundamental and harmonics of the pulse signal. This is easy to see with a spectrum analyzer. These “spurs” are very powerful and can saturate the LNA used to amplify the phase noise, which is low by nature, to the operating input level of the A/D converter. A filter, called video or PRF filter, will be connected between the phase detector output and the LNA input. The optimized cut-off value for this filter is half of the PRF, because this is the useful frequency range of a pulsed signal without aliasing problems.

DC offset of the detected phase noise signal

When the reference source is in CW mode and the DUT is on pulse, the DC offset voltage at the output of the phase detector can be larger than the useful beat signal. Sometimes this beat signal never crosses the zero voltage needed to calibrate and to lock the reference. The PN9000 software includes a special function (DC offset compensation) to solve this problem
Using a reference source in CW mode is very useful because this simplifies the operating mode. There is no need to pulse and trigger the reference.

Measurement advice

In addition to the above phenomena, the jitter (or phase noise) of the pulse generator can contribute to increase the noise of the pulse modulated signal, although this is difficult to quantify.
The PN9815 option, a single slot module, has been designed to prevent this problem. It includes two functions: a pulse generator and a microwave pulse modulator.
The pulse generator is driven from of a crystal oscillator and digital circuits to adjust PRF and duty cycle from the PN9000 software. The use of the PN9815 is strongly recommended to generate a low noise pulse waveforms.

The microwave pulse modulator, driven by the pulse generator, can be used for two purposes: to generate a pulsed signal from a CW signal and to generate a pulse window allowing measurement with a shorter duration than the initial DUT pulse. Example: if the noise contribution of the rising and falling edge has to be removed, the PN9815 can be programmed with a smaller pulse width in order to remove this part of the initial pulse.

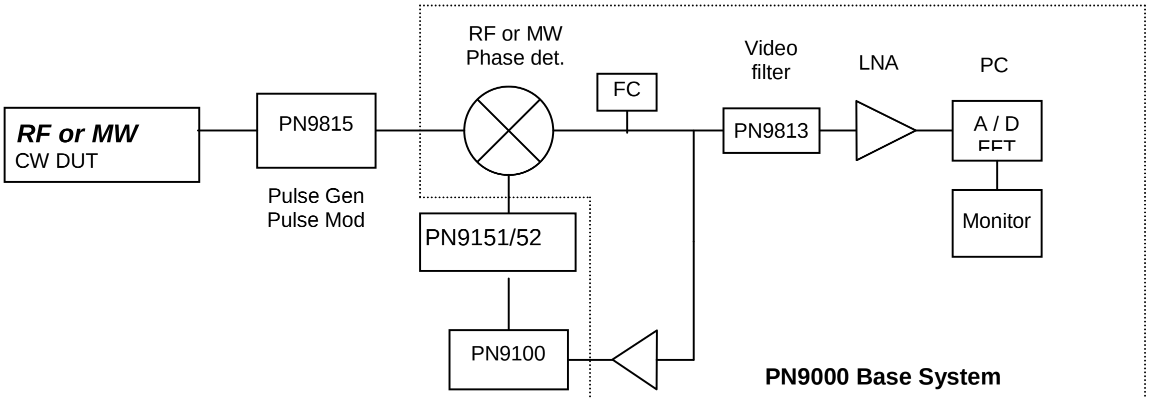
The PN9813 option, a single slot module, offers 5 video filter values, selected from the software. The values must be specified by the customer when ordering the system. Additional values can be provided in a second module, at any time.

The PN9341 phase detector option must be used, because it includes the SMA connectors on the front panel to connect the video filter.

Care must be taken about the increase of the residual noise due to power reduction. For example, if the MW phase detector is used, base system residual noise is – 165 dBc/Hz at 10 kHz offset with + 6 dBm CW RF and LO inputs. With a 10% duty cycle pulsed CW signal, the base system residual noise will increase by 20 dB, i.e. – 145 dBc/Hz, which still measures very clean radar sources. With a 1% duty cycle it will be reduced to – 125 dBc/Hz.

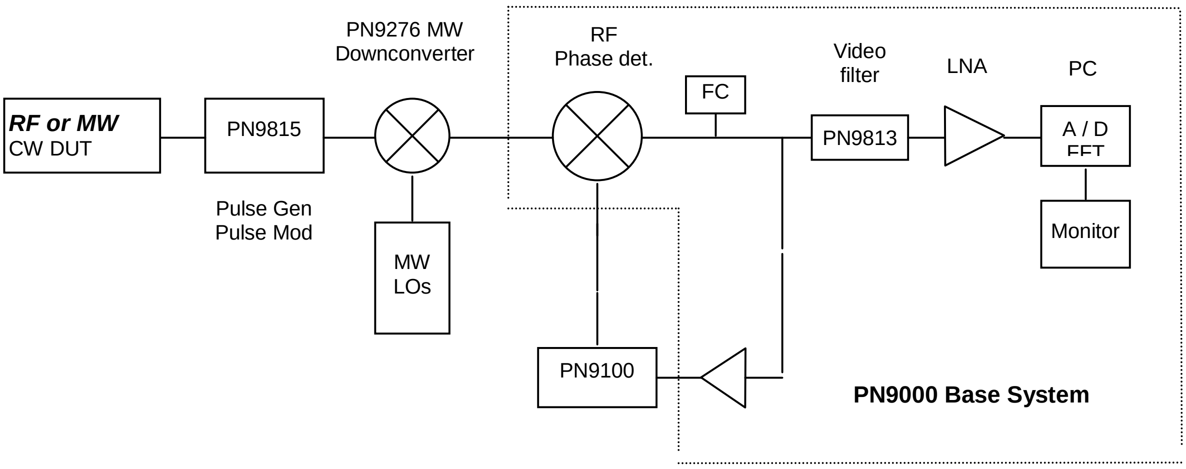
Measurement Methods

RF or MW DUT with Direct Phase Noise detection



This diagram will be used for RF source measurements up to 1.8 GHz with the standard RF phase detector and with the MW phase detector up to 4.5, 9.0 and 18.0 GHz depending on the PN9100 options implemented in the system.

MW signal down converted to the RF Frequency range



This method uses a MW down converter, PN9276, to down-convert the MW DUT signal to the RF frequency range of the PN9000 base system. This configuration, used for low noise MW source phase noise measurements, provides two advantages:

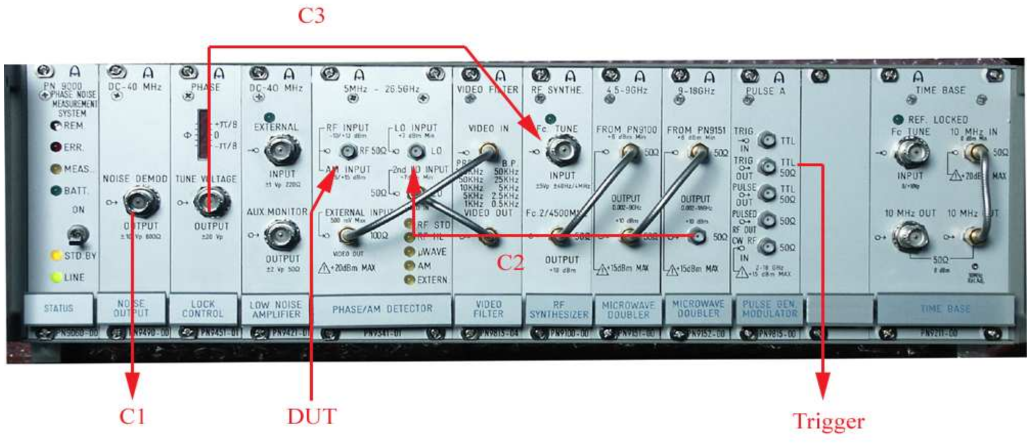
- Lower residual noise (noise floor), see the PN9276 datasheets for the specs,
- The built-in counter will measure RF, LO inputs and IF beat output of the standard RF phase detector. This makes LO tuning to the RF input frequency much easier.

If the DUT is already a pulsed signal, the PN9815 can be removed, but the pulse generator waveform of the PN9815 can still be used to drive the DUT pulse modulator.

Video filters specifications:

- Filter type : Low-pass , 4 or 6 poles
- Load impedance : 200 Ohms
- Cut-off frequency : ½ PRF (pulse repetition frequency)

The video filters are used to reduce the PRF spurs during the spectral analysis of the pulsed phase noise. 40dB attenuation of the PRF is needed, to not saturate the low noise amplifier.
The valid span analysis is half the PRF, example PRF= 100KHz, use the video filter 50KHz in the menu "System/Pulse". The valid span analysis is then 50KHz.



Example of a configuration with direct phase noise detection

Note: The PN9100 output is connected to the input of a PN9151 doubler, extending the range of the PN9100 to 9.0 GHz. A PN9152 would extend it to 18 GHz. Obviously, if the configuration includes a MW down converter, the PN9100 output is connected directly to the LO input of the phase detector.

The DUT signal is already pulse modulated
In that case, the DUT signal will be connected to the Phase detector input, in case of direct phase noise detection, or to the MW DUT input when a down converter is used. Then it is possible to use the PN9815 to pulse modulate the LO reference also. This has the advantage to suppress the DC offset. The PN9815 will use an external trigger and delays will be used to synchronize the RF and LO pulses. The duration of the two pulses must be the same. A dual trace scope might be necessary to achieve these adjustments. For more details, see the PN9815 datasheet.